

Bit-detection arrangement and apparatus for reproducing information

The invention relates to a bit-detection arrangement able to convert an analog signal having an amplitude into a digital signal representing a bit sequence from which the analog signal is derived, comprising:

- a quantizer able to produce an output signal S_1 by quantizing the amplitude of the analog signal, and
 - a phase detector PD_1 able to determine a phase difference ΔP_1 between the output signal S_1 and a clock signal C_2 , and able to generate an output signal PH_2 having an amplitude, where the amplitude of PH_2 indicates the phase difference ΔP_1 ,
 - an analog to digital converter ADC which is able to output a processed signal by sampling the output signal PH_2 at a sample rate controlled by a clock signal C_1 having a frequency which is equal to the frequency of clock signal C_2 divided by a factor n ,
 - a digital phase locked loop DPPLL able to lock on the processed signal and able to output a phase signal PH_1 using the clock signal C_1 , and
 - a bit decision unit able to output the digital signal and a clock signal C_3 using the phase signal PH_1 , the clock signal C_1 and the output signal S_1 , comprising a sample and hold unit SH_1 able to sample the output signal S_1 , using a clock signal C_{SH_1} having a frequency equal to the frequency of clock signal C_2 , and to hold n samples, sample_{y=1} through sample_{y=n}, of the output signal S_1 for a clock period of clock signal C_1 , n being the division factor of clock signal C_2 , where n is an integer greater than one.
- 20 The invention also relates to an apparatus for reproducing information recorded on an information carrier, having such a bit-detection arrangement.

From European Patent Application 0342736 a bit-detection arrangement is known which converts the analog signal into the processed signal by using the analog to digital converter ADC of the preprocessing unit. The processed signal thus comprises samples of the analog signal. The analog to digital converter ADC is controlled by the clock signal C_1 , which has a frequency of approximately the bit rate or greater of the bit sequence from which the analog signal is derived. The bits in the bit sequence will hereinafter also be

referred to as channel bits. The bit rate of the channel bits in the analog signal will hereinafter also be referred to as the channel bit rate, or the channel bit frequency. The digital PLL is able to output the phase signal PH_1 which indicates the phase difference between output signal S_1 and clock signal C_2 . The bit decision unit is able to determine a first crossing with a predetermined level of the phase signal PH_1 , and is able to output the digital signal by determining a sign of a sample of the analog signal at an instant in time in the neighborhood of the first crossing by using the processed signal. Therefore, in this case, the processed signal is used as signal S_1 mentioned in the opening paragraph. The bit decision unit is able to output the clock signal C_3 which is synchronous with the digital data. Clock signal C_3 is derived from the phase signal PH_1 . Clock signal C_3 is used to clock out the correct bits at the correct moments. The known bit-detection arrangement also comprises an interpolator which determines the phase difference between a zero crossing of the clock signal C_1 and a zero crossing of the processed signal. According to this phase difference the phase of the processed signal is corrected and subsequently fed to the digital PLL.

It is apparent that the analog to digital converter ADC has to sample at a rate determined by the channel bit rate. With increasing demands on the channel bit rate, the analog to digital converter ADC also has to sample at increasing rates. It is a drawback of the known bit-detection arrangement that it is not able to process analog signals with relatively high channel bit rates. Furthermore, an analog to digital converter ADC that can sample with relatively high sample rates is relatively expensive. Also the speed at which the digital PLL operates is determined by the channel bit rate, and therefore the demands on the digital PLL become higher with increasing channel bit rates.

Also an embodiment of a bit-detection arrangement is described in the not previously published PCT application IB02/04486 (PHN 14.010), further referred to as D1. The bit-detection arrangement described in D1 works as follows.

The output signal PH_2 of the phase detector PD_1 has a relatively low frequency if the difference of the frequency of the clock signal C_2 and the output signal S_1 is relatively small. Therefore the analog to digital converter ADC can sample at a relatively slow rate, and thus the ADC may be a relatively simple and inexpensive one. For this reason the clock signal C_1 may have a lower frequency than clock signal C_2 , in fact clock signal C_1 is derived from clock signal C_2 by dividing the frequency of clock signal C_2 by a factor n. The analog to digital converter ADC is able to use the clock signal C_1 to control the sample rate, resulting in the processed signal.

The quantizer quantizes the analog signal. A common used quantizer is a threshold detector. The threshold detector converts the analog signal into a digital signal. If the analog signal is above a predetermined threshold level, then the output signal S_1 has a value 1. Otherwise the output signal has a value 0. The sample and hold unit now can sample these 0's and 1's. Also the phase detector PD_1 can be implemented digitally, which has great advantages in that the phase detector is easily scalable, i.e. it automatically scales with changing clock pulse.

The bit decision unit is able to use the phase signal PH_1 to produce the digital signal which is synchronous in relation to the channel bits, thereby being able to use the 10 clock signal C_1 to output the digital signal. The sample and hold unit is capable of holding n samples. This unit is read out every cycle of clock signal C_1 , and during each cycle of clock signal C_1 there are n cycles of clock signal C_{SH1} . The n samples comprise a number of channel bits which number is dependent on the ratio of the channel bit frequency and the frequency of clock signal C_2 . For instance, if the frequency of clock signal C_2 is 15 approximately equal to the channel bit frequency, then the n samples comprise n channel bits. If the frequency of clock signal C_{SH1} is one and a half times the channel bit frequency, then the n samples comprise $2n/3$ channel bits. If, with this ratio, n equals 3, then 3 samples contain 2 channel bits.

So, one sample may contain a duplicate value of a channel bit which is already 20 represented by an other sample. If the phase difference exceeds a predetermined value, then the corresponding sample is the sample that may contain a duplicate value and the bit decision unit may decide not to output that sample in the digital signal. The decision not to output a sample will hereinafter also be referred to as discarding a sample. Because the amplitude of the processed signal represents the phase difference, it can be determined from 25 the processed signal which sample to discard. Because the digital phase locked loop locks to the processed signal, also signal PH_1 may be used for determining which sample to use and which sample to discard. Initial, the phase difference and thus the amplitude of PH_1 may start from zero. When the amplitude exceeds a predetermined value then a corresponding sample 30 may be discarded. The corresponding sample may be the sample closest to the point in time where the predetermined value is crossed. After that crossing, every time a multiple of the predetermined value is crossed, a corresponding sample may be discarded.

If the frequency of clock signal C_2 is approximately equal to the channel bit frequency, then the frequency of the processed signal is relatively low. Then also PH_1 has a relatively low frequency. Because the amplitude of PH_1 is only known at sampling instants

determined by clock signal C₁, the amplitudes of PH₁ corresponding to the samples of S₁ have to be determined, e.g. by interpolating the amplitude at the n sampling instants. This results in the amplitude of PH₁ at n points between each cycle of clock signal C₁. If the amplitude of PH₁ at one of the n points exceeds a multiple of the predetermined value, then 5 the corresponding sample of S₁ may be discarded.

If the frequency of PH₁ is relatively low, then the moments at which the amplitude of PH₁ exceeds a multiple of the predetermined value are relatively rare. This results in almost every sample of S₁ being outputted into the digital signal. This is the desired result, because when the frequency of PH₁ is relatively low, the frequency of the clock signal 10 C₂ and the channel bit rate is approximately the same. If those frequencies are exactly the same, then all samples are outputted.

If the frequency of PH₁ is relatively high, then the moments at which the amplitude of PH₁ exceeds a multiple of the predetermined value are relatively frequent. This results in a smaller number of samples of S₁ being outputted into the digital signal between 15 two subsequent cycles of clock signal C₁.

If n equals one, then the analog to digital converter ADC samples at the same speed as the analog to digital converter ADC of the known bit detection arrangement. Thus when n equals one the objective of the invention is not achieved. The clock signal that is fed to the digital phase locked loop DPLL and the bit decision unit does not explicitly has to be 20 clock signal C₁. A clock signal that fulfills the Nyquist criterion for the processed signal will suffice. Because clock signal C₂ always has a higher rate than clock signal C₁, clock signal C₂ may be used instead of clock signal C₁ in case of the digital phase locked loop DPLL and the bit decision unit.

With the bit detection arrangement described in D1, bits have to be discarded. 25 This is due to the fact that the sample frequency always has to be higher than the channel bit frequency, resulting in too many output samples. Therefore bits have to be discarded. The method to discard bits works correctly for data without phase jitter, but bit errors occur when jitter is present. When the sample moments and bit decision moments exactly match, maximum phase jitter is allowed. When the sample moments are exactly in between two bit 30 decision moments, no phase jitter is allowed.

It is a first object of the invention to provide a bit-detection arrangement of the kind described in the opening paragraph, wherein the allowable phase jitter is increased.

It is a second object of the invention to provide an apparatus for reproducing information recorded on an information carrier, which is provided with such a bit-detection arrangement.

- The first object is realized in that the bit decision unit further comprises
- 5 - at least one additional sample and hold unit SH₂ able to sample the output signal S₁, using a clock signal C_{SH2} and wherein the frequency of the clock signal C_{SH2} is equal to the frequency of clock signal C_{SH1} and the phase of clock signal C_{SH2} is substantially different from the phase of clock signal C_{SH1}, and
 - an output unit for outputting samples of either the sample and hold units SH₁ or SH₂, wherein the samples of the sample and hold unit SH₁ are outputted when the phase signal PH₁ indicates that the phase difference ΔP₁ is in a first region and the samples of the additional sample and hold unit SH₂ are outputted when the phase signal PH₁ indicates that the phase difference ΔP₁ is in a second region.

The bit detection arrangement according to the invention has at least two sample and hold units which sample the output signal S₁ and wherein one sample and hold unit uses clock signal C_{SH1} to sample the output signal S₁ and one sample and hold unit uses clock signal C_{SH2} to sample the output signal S₁. The clock signals C_{SH1} and C_{SH2} have the same frequency, but the phase of these clock signal is different. For instance the phase difference between clock signals C_{SH1} and C_{SH2} can be 180 degrees. If the phase signal PH₁ indicates that the phase difference between the clock signal C₂ and the output signal S₁ is around 0 degrees, than the samples of the sample and hold unit are outputted which is controlled with the clock signal having the smallest phase difference with clock signal C₂. If for instance clock signal C_{SH1} has the same phase as clock signal C₂ then the samples of sample and hold unit SH₁ are outputted. In that case the clock signal C_{SH2} can best be selected to have 180 degrees phase difference with clock signal C₂. Then, when the phase signal PH₁ indicates that the phase difference between the clock signal C₂ and the output signal S₁ is around 180 degrees, then the samples of the sample and hold unit SH₂ are outputted. This has the advantage that the phase jitter can be higher and still no bit errors occur. The first region in the above mentioned example is set to 0 to 90 degrees, and the second region to 90 to 180 degrees.

In a further embodiment of the bit-detection arrangement the bit decision unit further comprises sample and hold units SH₃ through SH_x, wherein the sample and hold units SH₁ through SH_x are clocked by clock signals C_{SH1} through C_x, wherein the frequency of the clock signals C_{SH2} through C_{SHx} is equal to the frequency of clock signal C_{SH1} and the phases

of the clock signals C_{SH1} through C_{SHx} are substantially different from each other and in that the output unit is adapted to output samples of the sample and hold units SH_1 through SH_x , wherein the phase signal PH_1 is divided into x regions, x being the number of sample and hold units, and wherein the output unit is able to output samples of the sample and hold unit
5 which corresponds to the region in which the current value of the phase signal PH_1 resides.

This has the advantage that the sample of output signal S_1 are sampled more accurately, i.e. the sample moment is can be chosen optimal. In the case that there are only two sample and hold units the sample moment can be maximal 90 degrees from the optimal sample moment. This results in that the maximum allowed phase jitter is reduced. By having
10 more sample and hold units, the sample moments can be chosen such that the maximum allowed phase jitter is increased compared to the embodiment with two sample and hold units.

In an other embodiment of the bit-detection arrangement according to the invention the bit detection unit further comprises a clock signal selection unit for outputting
15 the clock signal C_{SH1} and clock signal C_{SH2} wherein the clock signal selection unit is able to change the phases of the clock signals C_{SH1} and C_{SH2} in dependence of the current value of the phase signal PH_1 .

In this embodiment the phase of the clock signals C_{SH1} and C_{SH2} can be changed such that the sample moments are optimal with regard to the phase jitter. For
20 instance, when the phase signal PH_1 indicates that the phase difference ΔP_1 is between 0 and 45 degrees, the phase of the clock signal C_{SH1} is set to 22.5 degrees, and sample and hold unit SH_1 is used to sample. If the phase signal PH_1 indicates that the phase difference ΔP_1 is between 45 and 90 degrees the clock signal C_{SH2} is set to 67.5 degrees, and hold unit SH_1 is used to sample. Then for 90 to 135 degrees the phase of clock signal C_{SH1} is set to 112.5 degrees. Generally, the phase of the clock signal C_{SH1} is set to the middle of the current
25 region of the phase difference ΔP_1 . The phase of clock signal C_{SH2} can already be set beforehand, so that at the moment the phase signal PH_1 indicates that the phase difference ΔP_1 passes the 45 degrees, there can be directly switched from sample and hold unit SH_1 to sample and hold unit SH_2 .

30 In a further embodiment the clock signal selection unit is fed with clock signals C_1 through C_x having a frequency equal to clock signal C_2 and wherein the phases of the clock signals C_1 through C_x differ from each other, and wherein the clock signal selection unit passes two of the clock clock signals C_1 through C_x through as the clock signals C_{SH1} and C_{SH2} in dependence of the phase signal PH_1 .

In this embodiment the clock signal selection unit can easily change the phase of the clock signals C_{SH1} and C_{SH2} by selecting one of the clock signals C_1 through C_8 .

Instead of having two sample and hold units it is possible to have only one sample and hold unit and still be able to change the phase at which samples are taken. In the 5 embodiment with the clock signal selection unit the phase of the clock signal which clocks the one sample and hold unit, the phase is changed in dependence of the phase signal PH_1 . Directly switching between sampling moments when the phase signal PH_1 passes a certain value is then not possible. The sample and hold unit has already taken some samples with the clock signal having the previous phase. There is thus some delay before samples are 10 outputted from the sample and hold unit with the correct sample moments. This shows the advantage of having at least two sample and hold units.

The second object of the invention is realized in that the apparatus for reproducing information recorded on an information carrier is provided with the bit-detection arrangement according to the invention.

15 Such an apparatus generally also comprises:
a read head able to read information from the information carrier;
a displacement means able to cause a relative displacement between the information carrier and the read head;
a signal processing unit able to process a signal coming from the read head
20 into the analog signal;
a channel decoding means able to decode the digital signal.

The apparatus for reproducing information on an information carrier is able to use a bit-detection arrangement having an analog to digital converter with a relative slow sampling rate.

25 These and other aspects of the bit-detection arrangement and of the apparatus for reproducing information according to the invention will be apparent from and elucidated by means of the drawings, in which:
30 Fig. 1 shows an embodiment of the bit-detection arrangement described in not previously published PCT application IB02/04486;
Fig. 2a shows an example of the analog signal;
Fig. 2b shows a signal that represents the channel bit rate in the example of Figure 2a;

Fig. 2c shows the clock signal C₂ in the example of Figure 2a;

Fig. 2d shows the output signal PH₂ in the example of Figure 2a;

Fig. 3 shows an example of the processed signal in relation to the clock signals C₁ and C₂;

5 Fig. 4 shows an embodiment of a DPLL which is able to output a phase signal PH₂ which comprises 8 components indicating which of the 8 samples is valid;

Fig. 5a shows an example of the feedback signal in relation to the processed signal;

10 Fig. 5b shows another example of the feedback signal in relation to the processed signal;

Fig. 6 shows possible embodiments of the bit-detection arrangement comprising a frequency detector and a voltage controlled oscillator;

Fig. 7 shows an embodiment of the bit-detection arrangement comprising a location determining means;

15 Fig. 8a shows an example of the output signal S₁ in relation to the sample moments of clock signal C₂, where a sample is taken before zero crossing;

Fig. 8b shows an example of the output signal S₁ in relation to the sample moments of clock signal C₂, where a sample is taken after zero crossing;

20 Fig. 9 shows an embodiment of the bit detection arrangement using inverting means;

Fig. 10a shows an example of the phase difference ΔP₁;

Fig. 10b shows the output signal PH₂ when using the first inverting means in case of the phase difference ΔP₁ shown in Figure 10a;

25 Fig. 10c shows an example of the control signal in case of the phase difference ΔP₁ shown in Figure 10a;

Fig. 11 shows the relation between maximum allowed phase jitter and the phase difference ΔP₁;

Fig. 12a shows an example of the clock signal C_{SH1};

30 Fig. 12b shows an example of the analog signal with sampling moments with respect to the clock signal C_{SH1} of Fig.13a;

Fig. 12c shows an example of the clock signal C_{SH2};

Fig. 12d shows an example of the analog signal with sampling moments with respect to the clock signal C_{SH2} of Fig.13c;

Fig. 12e shows the phase signal PH₁ corresponding with Figures 12a to 12d;

Fig. 13 shows an embodiment of the bit detection unit of the bit-detection arrangement according to the invention;

Fig. 14 shows an other embodiment of the bit detection unit of the bit-detection arrangement according to the invention; and

5 Fig. 15 shows an embodiment of an apparatus for reproducing information provided with a bit-detection arrangement of the invention.

In the embodiment of the bit-detection arrangement shown in Figure 1 the
10 analog signal AS is converted into the processed signal PrS by the preprocessing unit 1. The digital phase locked loop DPLL 2 locks on to the processed signal PrS and outputs a phase signal PH₁. The bit decision unit outputs the digital signal DS and the clock signal C₃ using the phase signal PH₁, the clock signal C₁ and the output signal S₁. The clock divider 4 produces the clock signal C₁ by dividing the frequency of clock signal C₂ by a factor n. The
15 quantizer 11 quantizes the amplitude of the analog signal AS and outputs the resulting signal S₁. The phase detector PD₁ 12 determines the phase difference ΔP₁ between the output signal S₁ and the clock signal C₂ and feeds the output signal PH₂ to the ADC. The ADC then samples the output signal PH₂ at a rate controlled by the clock signal C₁. The sample and hold unit 31 samples the output signal S₁ to obtain binary samples using the clock signal
20 C_{SH1}. Clock signal C_{SH1} in this case is identical to the clock signal C₂. At the end of a clock cycle of clock signal C₁ the sample and hold unit 31 contains n samples. The bit decision unit may output all these samples at the beginning of the next cycle of clock signal C₁, or it outputs a smaller selection of these samples. Some samples may be discarded.

In Figure 2a the analog signal AS 5 is shown together with a level 8. In the
25 next example an embodiment of the quantizer 11 is a threshold detector. A threshold detector interprets samples as a logic 1 if the value of the sample is above a predetermined level, and as a logic 0 if the value of the sample is under a predetermined level. The level 8 shown in figure 2a is the predetermined level. The sampling moments of clock signal C₂ are indicated by the circles 6. The sampling moments of the original data is indicated by the crosses 7. In
30 Figure 2b the rising edges of the pulses indicate the sampling moments corresponding to the crosses 7, i.e. this signal represents the channel bit rate. The rising edges of the pulses in Figure 2c indicate the sampling moments corresponding to the circles 6, i.e. this signal represents the clock signal C₂.

The channel bits contained in the analog signal AS of Figure 2a are 1111 0001. The data that the sample and hold unit contains after sampling the output signal S₁ is 1111 1 0001. It is clear that one channel bit is sampled twice. In this case the fifth bit, i.e. sample_{y=5}, that the sample and hold unit 31 contains, may be discarded.

5 Further in Figure 2d it is apparent that the output signal PH₂, indicated by the solid line, has a relatively low frequency compared to the channel bit rate. The ADC 13 may sample at a relatively low rate. The output signal PH₂ is noisy because of disturbance in the channel bit rate e.g. due to jitter, mastering clock variations, etc. and because the phase difference ΔP_1 does not exactly have a linear course. Therefore also the processed signal PrS
10 is noisy because it is a sampled version of the output signal PH₂. The digital PLL 2 smoothes the processed signal PrS in order to oppress these disturbances.

As can be seen from the Figures 2a to 2d, at a first point the phase difference between the clock signal C₂ and the channel bit rate becomes so great that one channel bit is sampled twice. This first point corresponds to a second point at which the amplitude of the
15 output signal PH₂ crosses a predetermined value. Because ADC 13 samples at a clock cycle which is n times slower than the clock cycle of clock signal C₂, it is not clear from the processed signal PrS which of the n samples that the sample and hold unit 31 contains may be discarded. As shown in Figure 3 however, the processed signal PrS may be interpolated to obtain information about which sample may be discarded. The first sample corresponding to
20 the interpolation that is greater than the predetermined level L, may be discarded. A next sample may be discarded that has a corresponding interpolation that is greater than twice the predetermined value L. If the processed signal PrS at some point returns to zero, than of course the criterion for discarding the next sample is crossing the predetermined level L. In Figure 3 C₁ and C₂ are the cycles of the corresponding clock signals. If the embodiment of
25 the digital PLL 2 outputs a similar signal as the processed signal PrS, then instead of the processed signal PrS also the phase signal PH₁ may be used. In that case the interpolation may be done by the bit detection unit 3.

In Figure 4 the phase detector 21 outputs a phase difference signal ΔP_2 which is filtered by the integrating low pass filter 22. The filtered signal FS is fed to the
30 multiplicators 231 through 238. The multiplied signals are fed to the summators 241 through 248. The summated signals SUM₁ through SUM₈ are then fed to the truncator 25. The summated signal SUM₈ is truncated by the truncator and then fed as the truncated signal T_S to the buffer 26. Truncating in this context means resetting all bits in a bit presentation of the summated signal SUM₈ which are more significant than k least significant bits in the bit

presentation. If the summated signal SUM_8 of DTO_8 has a value of decimal 83, then a bit presentation of that sample of 8 bits is 0101 0011. If k equals 4 than the truncated signal T_rS sample equals 0000 0011, which represents decimal 3. The truncated signal T_rS is clocked into the buffer by clock signal C_1 , and outputted as the feedback signal FB for one clock cycle of C_1 . The feedback signal FB is added to the multiplied signals by the summators 241 through 248. Also the phase of the feedback signal FB is compared to the phase of the processed signal PrS by the phase detector 21. The phase signal PH_1 contains 8 components S_1V through S_8V . The signals S_1V through S_8V indicate which of the 8 samples is valid at a moment indicated by the clock signal C_1 . Hereinafter a value 1 of these signals indicate that 10 the corresponding sample is valid and may be outputted in the digital signal DS.

The DTO is clocked on frequency C_1 , which has a lower frequency than C_2 . A problem arises when a steep transition of the DTO is detected. Because of the slow DTO clock, it is not known which bit in the shift register has to be skipped. That is why DTO values are interpolated to determine more accurately where the steep transition took place.

15 Two methods for interpolating will be discussed.

The first interpolation method uses NC_2 number of DTOs. The inputs of the DTOs are multiplied with $1=NC_2$, $2=NC_2..$ ($NC_2+1)=NC_2$. When a DTO detects an overflow, while the previous DTO does not overflow, a steep transition is detected and the bit corresponding to the steep transition has to be skipped.

20 The second interpolation method uses a look-up table. When successive DTO values are known and a steep transition is detected in between, the two DTO values are combined to an address for the look-up table. The data corresponding to the address indicates which bit has to be skipped. When the DTO exceeds its maximum value, it truncates and returns to its most negative value. A steep transition will never occur exactly on a C_2 - . 25 moment, so a choice has to be made between skipping the bit sampled before or after the steep transition. Which of these 2 bits has to be skipped is not relevant, because both bits will have the same value when no phase jitter is present.

In Figure 5a an example of the processed signal P_rS , the feedback signal FB and a signal representing the channel bit frequency $ChBf$ are shown, whereby n equals 8. On 30 the horizontal axis periods of clock signal C_1 and clock signal C_2 are inserted. The feedback signal FB and the processed signal P_rS are clocked with clock signal C_1 . Clock signal C_2 is included for illustration purposes. In this example the clock signal C_2 has a slightly higher frequency than the channel bit frequency $ChBf$. As a result, the processed signal P_rS is varying relatively slowly. At every clock period of clock signal C_1 the feedback signal FB is

- buffered. The phase detector PD₂ 21 tries to synchronize the feedback signal FB with the processed signal P_rS. If that is the case, then the momentary amplitude of the feedback signal FB is substantially equal to the amplitude of the processed signal P_rS. Because almost all samples obtained by the sample and hold unit 31 may be outputted in the digital signal DS,
- 5 bits k+1 of subsequent summated signals SUM_x are alternating. This means that the filtered signal FS has a relatively high value. If for example bit k+1 represents a decimal value of 256, then the filtered signal FS has a value of approximately 250. This causes bit k+1 of subsequent summated signals SUM_x through alternate, and the signals S₁V through S₈V have a value 1, indicating all the samples may be outputted.
- 10 In Figure 5b the channel bit frequency ChBf is substantially lower than the channel bit frequency ChBf of the example shown in Figure 5a. This causes the processed signal P_rS to vary more quickly. As a consequence the frequency of the feedback signal FB decreases in order to synchronize the feedback signal FB with the processed signal P_rS. The filtered signal FS is decreased in order to decrease the frequency of the feedback signal FB.
- 15 The filtered signal FS may, for instance, have a value of 200. At one point bit k+1 of subsequent summated signals SUM_x does not alternate, and the corresponding sample is not outputted.

In the embodiment depicted in Figure 6 the clock signal C₂ is produced by the voltage controlled oscillator VCO. The frequency detector produces the VCO voltage as a function of the frequency of the output signal PH₂, or the frequency of the processed signal P_rS, or the frequency of the output signal S₁. The voltage controlled oscillator VCO and the Frequency detector FD of an embodiment using the frequency of the output signal PH₂ or the output signal S₁, can be implemented with analog electronics. The frequency detector FD of an embodiment using the processed signal P_rS, is preferably implemented with digital circuitry, because the processed signal P_rS is digital. Also the relation between the VCO voltage and the frequency of the input signal of the frequency detector FD is dependent on the signal used as the input signal of the frequency detector FD. For instance, the output signal S₁ has a higher frequency than the processed signal P_rS.

The location determining means LDM in Figure 7 is able to determine the location of the zero crossing of the output signal S₁ and the location of the zero crossing of the clock signal C₂. If, as indicated in Figure 8a, the sample 6 is taken just before the zero crossing of the output signal S₁, then the value of the sample is 1. The corresponding channel bit 7 also has a value 1, so the sample has the correct value. If, as indicated in Figure 8b, the sample 6 is taken just after the zero crossing of the output signal, then the value of the sample

is 0. The value of the sample is thus incorrect and may be toggled. The location signal may indicate to the bit decision unit to toggle this sample. The location signal can for instance be a bit-stream with the same frequency as clock signal C_2 , but with value 0 if the corresponding bit is preferably not to be toggled and a value 1 if the corresponding bit is preferably to be
5 toggled.

In Figure 9 the output signal PH_2 is fed to an input of the first conversion means 14. The first inverted signal CvS_1 is fed to the analog to digital converter ADC 13. Also a control signal CS is generated by the first conversion means 14. The control signal CS is fed to the second conversion means 27. The second conversion means 27 uses the control
10 signal CS to put back the steep transitions.

In Figure 10a the output signal PH_2 exhibits several steep transitions. Between point P1 and point P2, as shown in Figure 10b, the output signal PH_2 is inverted, thereby removing the two steep transitions at the points P1 and P2. Also a control signal CS is generated as can be seen in Figure 10c. In this example the control signal CS contains pulses
15 at the steep transitions. The second conversion means 27 operate in a similar manner.

The maximum allowed phase jitter with the bit-detection arrangement described in D1 as a function of the phase difference ΔP_1 is shown in Fig.11. With a phase difference ΔP_1 of 0 degrees the maximum allowed phase jitter is 180 degrees. When the phase difference ΔP_1 is 180 degrees then the maximum allowed phase jitter is 0 degrees.

In Fig.12a an example of the clock signal C_{SH1} is shown. The corresponding sample moments with respect to the analog signal AS is indicated by the crosses 101 in Fig.12b. The optimal sample moments are indicated by the circles 100. The phase signal PH1 indicating the phase difference between clock signal C_2 and the output signal S_1 is shown in Fig.12e. In this example the clock signal C_{SH1} has a phase equal to the phase of clock signal
20 C_2 . As can be seen by the crosses 101 in Fig.12b, the first few sample moments dictated by clock signal C_{SH1} are far from optimal. In fact, there is a great chance of bit errors. A little phase jitter will cause already cause bit errors. If the phase signal PH1 is between 90 and 180 degrees then the sample moments dictated by clock signal C_{SH1} can give bit errors with a higher probability of occurrence in the presence of phase jitter. This also holds if the phase
25 signal PH1 is between -90 and -180 degrees. In both cases the phase difference between the clock signal C_2 and the output signal S_1 is between 90 and 180 degrees, but in one case clock signal C_2 is leading with respect to output signal S_1 , and in the other case clock signal C_2 is lagging. If the phase signal PH1 is between -90 and 90 degrees the sample moments dictated
30 by clock signal C_{SH1} are close to optimal.

The clock signal C_{SH2} in Fig.12d has a phase difference with respect to clock signal C_{SH1} of 180 degrees. In Fig.12d the sample moments dictated by clock signal C_{SH2} are indicated by the crosses 102. The first few sample moments are close to optimal. If the phase signal PH1 is between 90 and 180 degrees, or between -90 and -180 degrees the sample
5 moments dictated by clock signal C_{SH2} are close to optimal. If the phase signal PH1 is in the range of -90 and 90 degrees these sample moments are far from optimal and bit errors could occur.

In order to avoid the bit errors in the presence of phase jitter the bit decision unit of the bit detection arrangement according to the invention is provided with at least two
10 sample and hold units. An example of an embodiment of the bit decision unit is shown in Fig.13. Here the bit decision unit 3 comprises sample and hold units SH1 through SHx, wherein x is an integer greater than one. The most elementary embodiment comprises two sample and hold units SH1 and SH2. Dependent on the value of the phase signal PH1 samples of one of the sample and hold unit SH1 through SHx are outputted as the digital
15 signal DS. The output unit 40 selects one of the samples 41 coming from the sample and hold units SH1 through SHX in dependence of the phase signal PH1. The output unit 40 selects the samples to output sample by sample depending on the current value of the phase signal PH1. This can mean that for instance the first two samples to output are taken from sample
20 and hold unit SH1, the next two samples from sample and hold unit SH2, the next three samples from sample and hold unit SH1, and so on.

An other embodiment of the bit decision unit 3 in accordance with the invention is shown in Fig.14. Here the bit decision unit comprises two sample and hold units SH1 and SH2. The clock signals C_{SH1} and C_{SH2} are selected by the clock signal selection unit CSU from the clock signals C_1 through C_x . The frequency of the clock signal C_1 through
25 C_x is identical to the frequency of clock signal C_2 , but the phases of these clock signals differ from each other. In dependence of the value of the phase signal PH1 the clock signals C_{SH1} and C_{SH2} are each connected to one of the clock signals C_1 through C_x . One of the clock signals C_{SH1} and C_{SH2} is connected to the clock signal which has the optimal phase for the current value of the phase signal PH1. The other clock signal (C_{SH1} or C_{SH2}) is connected to the clock signal that has a phase which is optimal for the next region of the phase signal PH1.
30 What the next region will be can be easily predicted. The phase signal will generally have a linear progress.

In Figure 15 the displacement means 200 displaces the information carrier 100 relative to the read head 300. The signal processing unit 400 converts a signal coming from

the read head 300 into the analog signal AS. The read head 300 could for instance be a laser unit and a detector for detecting a laser beam reflected by the surface of the information carrier 100. The detector can contain four sub-detection areas. The signal processing unit 400 then performs a summation operation to the signals coming from the sub-detection areas. The 5 analog signal AS is subsequently converted to the digital signal DS by the bit detection arrangement 500 of the invention. Following that conversion, the channel decoding means 600 further decodes the digital signal DS. The digital signal DS can for instance be a EFM coded signal.

The bit-detection arrangement can be implemented in a number of applications 10 and the invention is not limited to the implementation in the apparatus for reproducing information recorded on an information carrier. The bit-detection arrangement can for instance also be implemented in communication applications in general. For instance in telecom applications. Nowadays there are innumerable applications that need bit detection functionality. Especially when high communication speeds are required the bit-detection 15 arrangement according to the invention is preferably used as it relaxes the demands on the A/D converter and still have a low bit error rate.